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Author's Index

- A**
- Abad Grau, M. 2334
 Abdelbar, A. 402
 Adachi, N. 1057
 Adachi, S. 651
 Aiken, J. 713
 Aiyad, R. 419
 Akamatsu, N. 686
 Albesano, D. 2190
 Allinson, N. 2277
 Almeida, L. 2224
 Altug, S. 1250
 Alvager, T. 1580
 Amaral, J. 1235
 Amaral, W. 1624
 Amari, S. 39, 1530, 2328
 Amin, A. 1743
 Anand, T. 1466
 Andersen, T. 1920
 Anderson, R. 1559
 Aranki, N. 598
 Arantes do Amaral, J. 1889
 Araujo, A. 474, 2057, 2378
 Ariyanto, A. 310
 Asai, H. 646, 1652, 2157
 Atiya, A. 419, 1101
 Auda, G. 1356
 Aweya, J. 140
 Azimi-Sadjadi, M. 177, 1732
- B**
- Babuska, R. 1613
 Back, B. 266
 Baig, A. 160
 Bakker, R. 2483
 Balachander, T. 1804
 Balicki, J. 1646
 Balkarey, Y. 938
 Bandiera, N. 457
 Bao, W. 367
 Barataud, D. 128
 Barcia, R. 425
 Baron, R. 1433
 Barreto, G. 2378
 Barreto, J. 2413
 Barrows, G. 525
 Bartfai, G. 1137
 Bartfi, G. 2352
 Basak, J. 18
 Base, A. 1516
 Bax, E. 1230
 Bebis, G. 1688, 1717
 Behnke, S. 820
 Beiu, V. 1321
 Benedek, S. 1438
 Bennani, Y. 322
 Bennet, K. 2396
 Berger, T. 784, 2175
 Bergius, P. 189
- Bersini, H. 2402
 Berthold, M. 441, 447
 Best, P. 587
 Beuschel, M. 2425
 Bharitkar, S. 1629
 Biachini, M. 1619
 Bianucci, A. 117
 Birattari, M. 2402
 Bischof, H. 2294
 Blasch, E. 2092
 Blue, J. 2396
 Bluff, K. 630
 Blumenstein, M. 1738
 Boa, P. 1667
 Boehme, H. 372
 Bollacker, K. 1404
 Bologna, G. 146
 Bolouri, H. 165
 Bondarenko, V. 1472
 Bonifacio Jr., J. 205
 Bontempi, G. 2402
 Boronowski, D. 1937
 Borschbach, M. 837
 Bortolozzi, F. 1700
 Borzenko, A. 2541
 Bosch, H. 1167
 Boussalis, H. 943
 Brakensiek, A. 372
 Branca, A. 1590
 Branston, N. 326
 Braumann, U. 372
 Braun, J. 2184
 Brdys, M. 958
 Brejl, M. 814
 Brotherton, T. 876
 Brown, V. 625
 Browne, R. 431
 Bruce, J. 2214
 Bucciarelli, P. 2312
 Burkhardt, S. 1810
 Butler, J. 69
- C**
- Caldwell, C. 980
 Caloba, L. 1889
 Calvert, D. 2507
 Campbell, S. 1498
 Campolucci, P. 384
 Campos, M. 763
 Canelo, G. 996
 Canian, A. 205
 Caponetto, R. 492
 Capparelli, F. 903
 Carlton, A. 1047
 Carpenter, G. 763
 Carvalho, A. 277
 Carvalho, A. 271
 Casasent, D. 1971
 Castillo, O. 106
 Cawley, G. 101
- Cesmeli, E. 2069
 Cha, E. 1162, 1883
 Chadderdon, G. 876
 Chae, S. 156
 Chai, C. 2122
 Chakravarti, S. 832
 Chan, L. 237
 Chan, L.-W. 96
 Chan, S. 657
 Chang, H. 735
 Chang, J. 1428
 Chang, K. 695
 Chang, M. 680
 Chassiakos, A. 943
 Chatelet, E. 226
 Chatwin, C. 2034
 Chau, P. 928
 Chehade, H. 128
 Chen, F. 1520
 Chen, K. 367, 619
 Chen, M. 1851
 Cheng, S. 980
 Cheng, Y. 2273
 Cherkassky, V. 843, 2258
 Chew, P. 891
 Chi, H. 367
 Chiarantoni, E. 1877, 2361
 Chiu, W.-M. 2447
 Cho, C. 12
 Cho, J. 581, 1883
 Cho, K. 569, 669
 Cho, S. 1916
 Choi, D. 2028
 Choi, H. 1943, 2098, 2122
 Choi, J. 245, 1799
 Choi, S. 537, 1673
 Choi, W. 2122
 Cholewo, T. 1074
 Chow, H.-F. 96
 Chow, M. 63, 1250
 Chow, M.-Y. 12
 Choy, I. 245
 Chua, L. 503
 Chuieh, T. 1428
 Chun Su, M. 2116
 Cichocki, A. 39
 Cilingiroglu, U. 553
 Ciobanu, A. 1188
 Cipriano, A. 1981
 Ciuca, I. 1218
 Ciungradi, B. 216
 Claesson, I. 2180
 Cloarec, G. 2513
 Cloete, I. 1150
 Cochofel, H. 963
 Coggins, K. 1760
 Cohen, A. 938
 Coleman, S. 625
 Corchado, J. 713
 Costa, M. 216
- Costin, H. 1188
 Cox, C. 1047
 Craddock, R. 1361, 1382
- D**
- D'Arbo Jr., H. 474
 da Silva, I. 1624
 Dagher, I. 1688, 1717
 Dagli, C. 295
 Dahl, M. 2180
 Damper, R. 2196
 Dandolini, G. 425
 Das, S. 1559
 Daud, T. 593
 Daxwanger, W. 2086
 De, R. 18
 de Arruda, L. 1624
 de Azevedo, F. 2413
 de Carvalho, A. 205
 de Carvalho, A. 1723
 De Castro, F. 1235
 De Castro, M. 1235
 de Castro Silva, L. 1932
 de Figueiredo, R. 690, 1002
 De Nicolao, G. 2407
 de Vries, R. 2104
 DeClaris, N. 171
 DeFigueiredo, R. 408
 Delgado, A. 2126
 Deng, C. 221
 Denham, M. 1541, 1547, 1575
 Di Lecce, V. 1877
 Dich, W. 1299
 Diepenhorst, M. 603, 2519
 Diercksen, G. 1299
 Dillon, T. 29
 Diniz, H. 271
 Distant, A. 1590
 Dobeck, G. 177
 Downs, T. 1661
 Doya, K. 1553
 Dracopoulos, D. 2081
 Draghici, S. 547
 Dreyfus, S. 2016
 Drummond, S. 211
 Dunin-Barkowski, W. 640
 Duong, T. 593
- E**
- Ebecken, N. 1889
 Eem, J. 1943
 Eki, Y. 2346
 El Moudni, A. 57
 El-Deredy, W. 326
 Elinson, M. 938
 Eltoft, T. 408
 Embrechts, M. 1438
 Emerson, R. 123
 Engelbrecht, A. 1150, 1608

Euliano, N. 1063
Evitkhov, M. 938

F

Fancourt, C. 2324
Fanelli, S. 1619
Feldkamp, L. 69, 598,
1816, 2262
Feldkamp, T. 598
Feng, M. 2288
Ferguson, A. 165
Fernandez, M. 1450
Fernandez, P. 101
Ferrandez, J. 541
Ferreira, P. 1261
Fiori, S. 854, 1332, 2312
Fischer, I. 441, 447
Fisher III, J. 1712
Fletcher, L. 1608
Fortuna, L. 492
Fracassi, G. 79
Franco, P. 1235
Frangakis, A. 1937
Freisleben, B. 837
French, V. 1580
Frolov, A. 520
Fu, H. 1754
Fu, L. 45
Fu, M. 918, 1727
Fujimura, K. 301
Fujita, A. 1460
Fukao, T. 1057
Fukumi, M. 686
Fukushima, K. 1172
Furukashi, T. 35
Furukawa, S. 2306
Fyfe, C. 713

G

Gan, Q. 1156, 1293
Gao, X. 1954
Garavaglia, S. 289
Gauthier, F. 425
Geczy, P. 51
Gedeon, T. 343
Gemello, R. 2190
Georgiopoulos, M. 396, 1688,
1717
Ghosh, J. 695, 757, 1404
Gierczak, C. 69
Giles, C. 1051, 1834, 2483
Girau, B. 1433
Gobel, R. 1810
Goddu, G. 63
Gomez, J. 1564
Gomez, P. 541
Gomez-Ramirez, E. 390
Gomide, F. 251
Goncalves, R. 251
Gorban, A. 1271
Gori, M. 1619

Grabec, I. 1960
Grassi, G. 1504
Grbic, N. 2180
Gross, H. 372, 1992
Grudzinski, K. 1299
Gu, X. 1899
Guan, L. 922
Gubina, F. 1966
Guerriero, A. 1877
Guo, H. 1816
Guo, P. 725
Gutta, S. 1766

H

Ha, K. 1893
Haese, K. 1007
Hagen, C. 837
Hagiwara, M. 514, 1107,
1510
Hahnloser, R. 2373
Halgamuge, S. 7
Halilcevic, S. 1966
Ham, B. 134
Hamagishi, H. 1948, 2535
Hamalainen, J. 193
Han, J. 1667
Hangl, F. 2425
Haouani, M. 57
Hara, K. 2247
Hardier, G. 2441
Harkouss, Y. 128
Harris, P. 112
Haselsteiner, E. 1245
Hassoun, M. 486
Hatano, F. 609
Hattori, D. 1948
Hattori, M. 531
He, Y. 1388, 1478
He, Z. 221
Healy, M. 396
Heh, J. 680
Heileman, G. 396, 1688, 1717
Herault, L. 1239, 1398
Hernandez, C. 1450
Hernandez Molinero, L. 2334
Heywood, M. 2034
Hikawa, H. 557
Hikosaka, O. 1553
Hirabayashi, A. 2236
Hirasawa, K. 480, 968, 1482,
1602, 2346, 2453, 2465
Hirose, A. 1078
Ho, T. 1524
Hodge, L. 283
Holmstrom, L. 1305
Honavar, V. 2208, 2318
Hong, D. 537
Horne, B. 1051, 1834
Horst, P. 277
Hoti, F. 1305
Hou, Z. 1667
Howard, A. 231

Hoyer, P. 859
Hrycej, T. 949
Hu, J. 968, 1482, 1602,
2346, 2453, 2465
Hu-Yu, X. 1624
Huang, C. 2116
Huang, D. 1113
Huang, H. 2116
Huang, K. 1840
Huang, Q. 177
Huang, X. 497
Husek, D. 520
Hussain, T. 431
Hwang, H. 1799
Hyvarinen, A. 859, 1350,
2282

I

Ibikunle, F. 2557
Ibnkahla, M. 865
Ichigashi, H. 651
Ichihashi, H. 1224, 2390
Ichimura, T. 1131
Ikeda, K. 2340
Ikeda, M. 306
Ikeda, N. 486
Ikeda, T. 2306
Ilg, W. 1367
Ineyama, N. 1057
Intanagonwiwat, C. 462
Ioannou, P. 943
Ishibuchi, H. 2051
Ishikawa, M. 2328
Ito, K. 2367
Ito, N. 780
Iwanoto, K. 301
Iwasa, T. 992
Izhikevich, E. 2547

J

Jagielska, I. 24
James, J. 598
Janet, J. 2218
Jarvimaki, I. 193
Jayasuriya, A. 7
Jerry Lin, J. 1428
Jesion, G. 69, 598
Jiang, D. 1640
Jie, Z. 359
Jimenez, D. 753
Jo, T. 2531
Johnson, J. 2092
Johnson, J. 1784
Johnson, T. 876
Joshi, A. 211
Joutsensalo, J. 152

K

Kambhampati, C. 1361
Kamel, M. 1356, 2507
Kameyama, K. 1861

Kamimura, R. 1030, 1845
Kamo, A. 2157
Kanada, H. 2471
Kanata, Y. 1002
Kanerva, P. 1416
Kang, M. 1162
Karaf, A. 2247
Karayiannis, N. 2230
Kasatkina, L. 241, 1685
Kaski, S. 413
Katkovink, V. 1608
Kawakami, H. 2300
Kayama, M. 701
Keller, E. 1559
Khalaf, A. 1975
Khan, M. 262
Khorasani, K. 378, 2063
Khosla, R. 29
Kim, D. 1799
Kim, G.-S. 790
Kim, J. 134
Kim, K. 1883
Kim, S. 1943, 2122
Kimura, E. 1172
King, I. 237, 932
Kirby, S. 112
Kisdia, S. 301
Kita, H. 2010
Kitowski, Z. 1646
Kiviluoto, K. 189, 2268
Klopf, A. 2092
Koch, M. 441, 447
Kocher, M. 1047
Koivisto, H. 2419, 2477
Koivo, H. 2419, 2477
Kok, J. 730
Kolb, T. 1367
Konar, A. 747
Konishi, R. 1772
Kosmatopoulos, E. 943
Kosugi, Y. 349, 1861, 2471
Kothari, R. 1778, 1804
Kozek, T. 503
Krabbes, M. 372, 1992
Kruse, R. 468
Kuh, A. 1584
Kulczycki, P. 1344
Kumamaru, K. 2453, 2465
Kumayama, J. 701
Kung, S. 1051, 1834
Kuo, R. 90
Kuriyama, Y. 1131
Kuroe, Y. 2300
Kussul, E. 241, 1685
Kussul, N. 1685
Kusumoputro, B. 310
Kwon, H. 1799

L

L'Abbate, G. 1569
Labbi, A. 1167

Labonte, G. 880
Lai, Z. 725
Lamedica, R. 79
Lamers, M. 730
Lampinen, J. 199
Lancieri, L. 1454
Lane, C. 2163
Lang, S. 2151
Lange, J. 1810
Lappalainen, H. 2384
Lathia, B. 134
Lau, T. 932
Lebret, E. 730
Lee, B. 1916
Lee, C. 954
Lee, H. 2357
Lee, H.-M. 2447
Lee, H. 1943
Lee, I. 1799
Lee, J. 2028
Lee, K. 537
Lee, M. 2098
Lee, S. 613, 2122
Lee, S. 581, 2357
Lees, B. 713
Lefebvre, D. 57
Lendaris, G. 1013
Leonardis, A. 2294
Lepage, R. 1176
Lera, G. 2242
Leung, K. 2151
Leung, S. 1090
Levine, D. 625
Levkowitz, H. 2184
Lewis, C. 1047
Li, B. 63
Li, C. 1119
Li, G. 1857
Li, J. 359, 2092
Liang, X. 1388
Liaw, J. 2175
Liebe, C. 231
Lien, S. 1143
Lin, C. 2116
Lin, C. 2116
Lin, D. 1794
Lin, S. 353
Lin, T. 1051, 1834
Lindblad, T. 803
Lindsey, C. 803
Lindsey, D. 2069
Liou, R. 1851
Liqing, Z. 437
Lisboa, P. 112, 326
Liu, X. 897
Liu, Y. 2202
Lo, J. 1311, 2429
Lo, K. 74
Lobo, V. 457, 1910
Lopera, F. 1564
Lotlikar, R. 1778
Lu, H. 1478

Lu, T. 2131
Lu, W. 1857
Lu, Y. 1816
Lucas, S. 1867
Ludik, J. 1926
Luk, A. 1090, 1143
Luk, P. 1095, 1315, 1377
Lursinap, C. 1125
Lynn, G. 1488

M

Macchiarul, L. 216
Maeda, Y. 1002, 1772
Mak, M. 669
Makaruk, H. 1321
Makikallio, T. 797
Mana, F. 2190
Mandal, A. 747
Mandelj, S. 1960
Manzie, C. 986
Mao, J. 1828
Marino, C. 928
Marko, K. 598, 1286
Martin, T. 980
Martini, E. 271
Martinelli, G. 79
Martinez, T. 509, 1036, 1920
Martins, A. 425
Martins, W. 1932
Mascioli, F. 79
Mascolo, S. 1504
Mathur, S. 913
Matsuda, S. 1657
Matsumoto, T. 1948, 2535
Matsumoto, Y. 634
Matsushita, S. 35
Matsuyama, Y. 2306
May, E. 295
Mayosky, M. 996
McCabe, S. 1541, 1547, 1575
Meert, K. 719, 1926
Melin, P. 106
Mellgren, R. 625
Melnik, O. 1069
Mendel, J. 1629
Menozzi, A. 12
Mercado III, E. 1584
Michaelis, B. 707
Micheli, A. 117
Michiyuki, Y. 1748
Milanese, R. 1167
Minai, A. 587, 1466
Mirmirani, M. 943
Misawa, J. 1482
Mishra, Y. 913
Misra, M. 1327
Mitsui, M. 2300
Miyazaki, Y. 497
Miyoshi, S. 2340
Miyoshi, T. 651, 1224, 2390, 2390

Mizutani, E. 503, 2016
Mizutani, S. 2551
Montuno, D. 140
Moore, W. 2146
Moreira, E. 205
Mori, T. 2300
Morishta, T. 609
Morizumi, N. 992
Morooka, Y. 701
Moura-Pires, F. 457, 1910
Mouria-Beji, F. 1200
Mozayyani, N. 160
Murata, J. 480, 968, 1482, 1602, 2453, 2465
Murshed, N. 1700
Mutata, J. 2346

N

Na, K. 156
Nagano, S. 1553
Nakahara, H. 1553
Nakajima, Y. 1948
Nakashima, A. 2236
Nakashima, T. 2051
Nakayama, K. 1494, 1975, 2247, 2253, 2340
Nan, J. 2075
Nelson, A. 2489
Neville, R. 1095, 1315, 1377
Newcomb, R. 541
Ng, S. 1090
Ngoya, E. 128
Niestroy, M. 2110
Nijhuis, J. 603, 2519
Nikulin, V. 809
Ninomiya, H. 646, 1652, 2157
Nishikage, T. 634
Nishikawa, Y. 2010
Noda, T. 480
Noumeir, R. 1176
Nunes, L. 2224
Nurnberger, A. 468

O

Occhipinti, L. 492
Ogawa, H. 2236
Ogawa, T. 2471
Oh, C. 2051
Oh, H. 134
Oh, S. 2357
Oh, S. 2028
Ohbayashi, M. 968, 1482, 1602, 2346, 2465
Ohbayayshi, M. 2453
Ohkouchi, K. 1748
Ohsugi, M. 2253
Oja, E. 859, 2268
Okabe, Y. 2367
Oliveira, I. 1194
Omatu, S. 891, 909, 992, 2142

Onat, A. 2010
Ong, S. 537
Onishi, H. 1078
Onozuka, T. 2045
Orlov, Y. 938
Osaki, T. 663
Osana, Y. 514, 1107, 1510
Ota, Y. 2435, 2459
Oten, R. 690
Ouyang, N. 306
Owen, M. 1019

P

Pacheco, R. 425
Pacut, A. 2004
Padgett, C. 231
Padgett, M. 803, 1784
Padilha, T. 277
Pajunen, P. 152, 1350
Pal, S. 18
Palaniswami, M. 986, 1256
Panchapakesan, C. 1256
Pap, R. 1047
Paplinski, A. 1372
Paquir, W. 865
Paraskevopoulos, V. 2034
Parekh, R. 2208, 2318
Park, B. 1905
Park, C. 1883
Park, D. 826, 1673
Park, S. 958
Park, T. 826
Park, W. 1943
Park, Y. 569, 2098
Parlos, A. 1101
Pasero, E. 216
Pasquet, S. 226
Patel, R. 2063
Paul, B. 747
Peck, M. 101
Pellegrini, C. 146
Peng, H. 1293
Peng, P. 1147
Perez-Urbe, A. 2022
Perov, P. 938
Perry, L. 1873
Perry, S. 922
Peterson, T. 768
Piazza, F. 384, 903, 1332, 2312
Piazza, P. 854
Pinho, A. 870, 1261
Pinzolas, M. 2242
Pollack, J. 1069
Pozarkik, R. 1444
Poznyak, A. 390
Prampero, P. 1723
Principe, J. 849, 963, 1063, 1084, 1488, 1712, 1760, 2324
Privault, C. 1398

Prokhorov, D. 2262
 Protasi, M. 1619
 Prudenzi, A. 79
 Puskorius, G. 69, 598
 Putman, G. 1580

R

Rachkovskij, D. 241, 1685
 Radetzky, A. 468
 Ragheb, M. 337
 Raitz, R. 425
 Ralph, D. 1256
 Ramirez, J. 897
 Rampone, S. 774
 Ratto, G. 1569
 Raudys, S. 1530
 Raveendran, R. 891
 Ray, S. 337
 Rees, N. 713
 Regoli, M. 79
 Reinke, D. 1732
 Rezende, S. 271, 277
 Rhee, F. 1905
 Riberiro, B. 1987
 Riedmiller, M. 1998
 Rijckaert, M. 719, 1926
 Ringwood, J. 2513
 Rizzi, A. 79
 Roa, L. 541
 Rocha, C. 277
 Rodellar, V. 541
 Roisenberg, M. 2413
 Rojas, R. 820
 Roning, J. 797
 Roppel, T. 1784
 Rouat, J. 1524
 Rouhana, R. 1176
 Rousset, J. 128
 Rukonuzzaman, M. 74
 Ryosuke, K. 663

S

Sabala, I. 39
 Sabsich, T. 165
 Saeki, K. 1460
 Saeks, R. 1047
 Saez, J. 1981
 Saini, J. 913
 Saito, M. 1948, 2535
 Sanchez, E. 2022
 Sandberg, I. 1212, 1265
 Sano, T. 2551
 Sanz-Bobi, M. 1981
 Sarajedini, A. 928
 Sarkar, M. 741
 Schioler, H. 1344
 Schmidt, G. 2086
 Schouten, J. 2483
 Schroder, D. 2425
 Schultz, S. 2218
 Schunemann, S. 707

Scoggins, S. 2218
 Sefic, W. 1047
 Sekerkiran, B. 553
 Sekhar, C. 1206
 Sekine, Y. 1460
 Sellami, L. 541
 Seppala, J. 2419
 Sere, K. 266
 Setiawan, E. 832
 Sgro, J. 123
 Sha, L. 1293
 Shaheen, S. 419
 Shaibon, H. 74
 Shalvi, D. 171
 Shannon, T. 1013
 Shao, N. 1602
 Shao, X. 843
 Shepherd, R. 2258
 Sheu, B. 569, 784
 Shi, B. 1857
 Shi, D. 974
 Shibata, K. 2367
 Shimohara, K. 2551
 Shin, C. 1119
 Shin, S. 2357
 Shinchi, T. 1772
 Shishkin, S. 640
 Shouno, H. 1172
 Si, J. 353
 Sick, B. 84
 Simonetti, M. 384
 Singh, S. 1743
 Sio, K. 954
 Sipe, M. 1971
 Sirag, D. 1147
 Sjodin, G. 1410
 Smith, K. 1679
 Snijder, F. 1613
 Someya, K. 1460
 Song, J. 245
 Song, S. 1799
 Song, S. 2079
 Song, W. 2288
 Sonka, M. 814
 Souza, J. 425
 Spaanenburg, L. 603, 2519
 Speer, R. 2146
 Sperduti, A. 117
 Srivastava, M. 913
 Stacey, D. 283, 2507
 Stanton, P. 123
 Starita, A. 117, 1569
 Stassinopoulos, D. 2039
 Stateczny, A. 1646
 Steffens, F. 1608
 Stella, E. 1590
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 Stubberud, S. 1019
 Su, M. 735
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 Suddarth, S. 593

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 Suganthan, P. 1706
 Sugarhara, K. 663
 Sung, J. 1948, 2535
 Sugita, Y. 701
 Sukharev, A. 640
 Sun, K. 613
 Sun, P. 1286
 Sun, R. 1, 768
 Sun, W. 885
 Sundareshan, M. 1024, 2169
 Sung, A. 316
 Sutton III, J. 2218
 Swindell, R. 112
 Swiniarski, R. 1910
 Sze, H. 2151

T

T'sou, B. 657
 Tagliarini, G. 402
 Takeda, F. 634, 1748
 Takeda, N. 2306
 Talebi, H. 2063
 Talukder, A. 1971
 Tan, A. 183
 Tan, Y. 221
 Tanaka, H. 1224
 Tanaka, M. 1748
 Tanprasert, T. 1125
 Tavares, V. 1488
 Tawel, R. 598
 Teo, C. 183
 Ter Haseborg, H. 603
 Teramoto, I. 609
 Teyssier, J. 128
 Thakoor, A. 593
 Tham, M. 1361
 Thomas, D. 326
 Thomas, T. 593
 Tian, B. 177, 1732
 Todd, J. 2069
 Todirascu, A. 1188
 Togo, K. 1602
 Tokutaka, H. 301
 Tomikawa, Y. 1494
 Tontini, G. 1694
 Toshimitsu, K. 968
 Tranpraset, C. 1125
 Treadgold, N. 343
 Trecate, G. 2407
 Trussell, H. 1250
 Tsai, M. 1422
 Tsai, R. 784
 Tsai, W. 2447
 Tse, P. 2151
 Tso, S. 1899
 Tsutsui, H. 35
 Tulppo, M. 797
 Turner, K. 757

U

Uchikawa, Y. 780
 Uluyol, O. 337
 Uncini, A. 384, 854, 903
 Usui, S. 51
 Uto, K. 349

V

Vacca, F. 2361
 Vainamo, K. 797
 Van Bael, P. 719
 van den Bleek, C. 2483
 Van Gorp, J. 2136
 Vanharanta, H. 266
 Vanyachine, A. 803
 Vaucher, G. 160
 Vellido, A. 112
 Venema, R. 2519
 Ventura, D. 509, 1036
 Verhaegen, M. 1613
 Verma, B. 332, 1738, 1790, 2163
 Verzi, S. 396
 Vierira, M. 2057
 Visala, A. 1281
 Voigt, H. 1810
 Von Zuben, F. 251, 1932
 Vonder Haar, T. 1732
 Voronenko, D. 674

W

Wallace, J. 630
 Wams, B. 2104
 Wan, E. 2489
 Wang, C. 1084
 Wang, D. 619, 897, 1182, 1498, 2069
 Wang, F. 363
 Wang, G.-N. 790
 Wang, J. 885, 1422, 1596, 1640
 Wang, L. 1679
 Wang, T. 725
 Wang, Y. 1624
 Wangchao, L. 359
 Ware, J. 1218
 Warner, B. 1327
 Warwick, K. 1361, 1382
 Watanabe, E. 2501
 Watanabe, M. 780
 Watanabe, T. 301
 Watson, H. 986
 Watta, P. 486
 Wazlawick, R. 1194
 Wechler, H. 1766
 Wei, Y. 1293
 Wenjing, L. 359
 White, M. 2218
 White, R. 2352
 Wilamowski, B. 2435, 2459

PID Controller Design Using Dynamical Neural Networks

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1 abstract

In this paper, a new PID control scheme using neural networks is presented. The scheme is to parameterize a Ziegler-Nichols-like formula with a single parameter and use the dynamical neural networks to tune the parameter. A Lyapunov type stability criterion is derived to ensure the convergence of the neural procedure and guarantee the stability of the closed-loop system. The simulation examples with small and large time delay are given to illustrate the performance of the proposed method. Simulation results demonstrate that better control performance can be achieved when compared with that of the Ziegler-Nichols PID controllers and that of the fuzzy selftuning of PID control scheme.

2 Introduction

Despite the appearance of many sophisticated control theories and techniques, the majority of industrial processes nowadays still use the proportional-integral-derivative (PID) controllers, since their simple structure and easy implementation. However, a crucial issue for designing the PID controllers is how to set the control parameters. The conventional way to set them is by try and error method. It has been shown that the PID control scheme is adequate to achieve desired performance if the process is modeled perfectly and the load is not changed frequently. However, a real industrial process can never have such ideal properties and fixed loads. So

far, great effort has been devoted to developing methods for choosing the optimizing control parameters, especially for dealing with time-delay processes [1, 2]. In general, the control parameters of the PID controllers are usually selected to be fixed during control when they are tuned or chosen in a certain optimal way. However, such method cannot obtain effectively control performance since the control parameters can not be changed when the load disturbances change. Thus, it may always need frequently on-line re-tune in order to obtain good performance [3, 4, 5]. In this paper, a new PID control scheme using neural networks is presented. The scheme parameterizes the Ziegler-Nichols-like formula with a single control parameter and exploits the possibilities of the controllers for achieving better performance for the unknown systems with uncertainty or known structures with unknown variation in parameters due to the load disturbances. The control parameters are recursively learned from the error signal between the plant output and the reference input. The simulation examples with small and large time lags are given to illustrate the performance of the proposed method. From simulation results, better control performance can be expected by the proposed method than that of the PID controllers or that of the fuzzy selftuning of PID control scheme.

3 Problem Formulation

To begin with, we assume that the process to be controlled has single input $u(t)$ and single

output $y(t)$, and the control objective is to let the process output follow a prescribed set-point y_r . Let the tracking error be defined by

$$e(t) = y_r - y(t) \quad (1)$$

The PID controller, which generates the control signal, $u(t)$, has the following:

$$u(t) = K_c \left[e(t) + T_d \frac{de(t)}{dt} + \frac{1}{T} \int e(t) dt \right] \quad (2)$$

where K_c, T_d, T_i are three control parameters and are defined, respectively, as the proportional gain, the derivative time and the integral time of the controller. From [4], the control parameters can be parameterized by a single parameter α and are shown in the following

$$\begin{cases} K_c = 1.2\alpha k_u \\ T_i = 0.75 \frac{1}{1+\alpha} t_u \\ T_d = 0.25T_i \end{cases} \quad (3)$$

where k_u and t_u are the ultimate gain and the ultimate period of the underlying process respectively. The form of the parameterization is inspired by the Ziegler-Nichols formula when $\alpha = 0.5$. Thus, we can think of the controller as to improve the Ziegler-Nichols control scheme by biasing all the control parameters in order to control the process output to a prescribed signal.

In this paper, the $\alpha(t)$ is defined by the following dynamical equation

$$\dot{\alpha} = -\beta\alpha + \omega s(\alpha) \quad (4)$$

where β is a positive constant and ω is a weight. Let $s(\alpha)$ be a smooth (at least twice differentiable), monotone increasing function and be represented by sigmoids of the form

$$s(\alpha) = \frac{k}{1 + e^{l\alpha}} \quad (5)$$

where k, l are, respectively, parameters representing the bound and slop of sigmoid's curvature [6].

The purpose of the paper is to find the learning rule for weight, ω , such that the closed-loop system is stable and weight can converge to its true weight value, ω^* . We assume that ω^* exists, then, in the steady-state, (4) becomes

$$\dot{\alpha} = -\beta\alpha + \omega^* s \quad (6)$$

Let

$$h = \frac{1}{2}\alpha^2 \quad (7)$$

then

$$\begin{aligned} \dot{h} &= \frac{dh}{d\alpha} \dot{\alpha} \\ &= \alpha(-\beta\alpha + \omega^* s) \end{aligned} \quad (8)$$

Define

$$\dot{\eta} + \gamma\eta = -\dot{h} + \alpha(-\beta\alpha + \omega s) \quad (9)$$

where γ is some positive constant. Let the Lyapunov function candidate be defined by

$$V = \frac{1}{2}\eta^2 + \frac{1}{2}\tilde{\omega}^2 \quad (10)$$

where $\tilde{\omega} = \omega - \omega^*$. Differentiating (10) and using (9), we obtain

$$\dot{V} = -\gamma\eta^2 + \eta\alpha\tilde{\omega}s + \tilde{\omega}\dot{\tilde{\omega}} \quad (11)$$

If we choose

$$\dot{\tilde{\omega}} = \dot{\omega} = -\alpha\eta s \quad (12)$$

then (11) becomes

$$\dot{V} = -\gamma\eta^2 \quad (13)$$

Now we can prove the following theorem.

Theorem 1: Consider the Lyapunov function (10). The learning rule

$$\dot{\omega} = -\alpha\eta s \quad (14)$$

guarantees the following properties

- $\eta, \alpha, \tilde{\omega} \in L_\infty$
- $|\eta| \in L_2$
- $\lim_{t \rightarrow \infty} \eta = 0$
- $\lim_{t \rightarrow \infty} \tilde{\omega} = 0$

Proof: From (11) and (14), $\dot{V}$ becomes

$$\dot{V} = -\gamma \eta^2 < 0$$

Hence, $V \in L_\infty$, which implies $\eta, \tilde{\omega} \in L_\infty$. Since V is a nonincreasing function of time and is bounded from below, $\lim_{t \rightarrow \infty} V = V_\infty$ exists. Therefore by integrating $\dot{V}$ from 0 to ∞ , we have

$$\int_0^\infty \|\eta\|^2 dt = \frac{1}{\gamma} [V(0) - V(\infty)] < \infty$$

which implies that $\eta \in L_2$. By definition, the sigmoid function $s(\alpha)$ is bounded for all α and, by assumption, all inputs to the dynamical adaptation are also bounded. Hence, from (9), we have $\dot{\eta} \in L_\infty$. Since $\eta \in L_2 \cap L_\infty$ and $\dot{\eta} \in L_\infty$, using Barbalat's Lemma, we conclude that $\lim_{t \rightarrow \infty} \eta = 0$. Now using the boundedness of $s(\alpha)$ and the convergence of η to zero, we have that $\dot{\tilde{\omega}}$ also converges to zero.

4 Example

Let the controlled process with time delay be defined by

$$G(s) = \frac{k_p e^{-\theta_d s}}{(Ts + 1)^2} \quad (15)$$

The parameters k_p and T are all set to 1, and the dead-time, θ_d , will be set to two different values to examine the ability of the proposed control scheme in handling small or large dead-time. First, the value of θ_d is chosen to be 0.3 and y_r is set to be 1 to track a unit step signal, and the load disturbance, $0.2 \sin(t)$, is introduced when $t = 20$. The simulation results

are shown in *Figure 1 - Figure 4*. *Figure 3* shows the performance of the PID controller with dynamical neural network for the set-point response which is better than that of the other two controllers shown in *Figure 1* and *Figure 2* with shorter rise time, shorter setting time, and less overshoot. Observe that unlike other controllers where lowering the overshoot is often at the expense of slowing down considerably the rise time, the proposed control scheme seems to reconcile these two requirements. The reason is that the dynamical neural type PID controller allows the selection of different control parameters for controlling the process at every time interval. The controller is then designed so that it can pick up an appropriate performance at every control stage. Next, the value of θ_d is then set to be 0.8. The load disturbance, $0.2 \sin(t)$, is also introduced at $t = 20$ to allow the process to settle down. The simulation results are shown in *Figure 5 - Figure 8*. From *Figure 1 - Figure 3* and *Figure 5 - Figure 7*, we can conclude that the set-point response improves considerably while the responses are either comparable to those obtained by the conventional controllers (in the case of small dead-time), or only improves marginally (in the case of large dead-time).

5 Conclusions

In this paper, We have presented a detailed account of the PID controller using dynamical neural networks. One interesting feature of the present work is the combination of the conventional PID controller with the dynamical neural networks. Because of our scheme's connection with Ziegler-Nichols formula, the proposed control scheme is not completely model-free. We have provided a method to derive a learning rule for the weight of the neural networks such that the control parameters of the PID controller can be tuned properly whenever the load

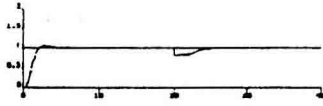


Figure 1: The response of the PID controller using the Ziegler- Nichols formula, where $K_c = 2.808$, $T_I = 1.64$, $T_d = 0.41$.



Figure 4: The parameter α .

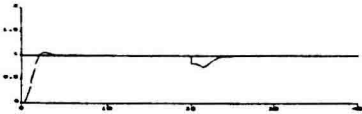


Figure 2: The response of the fuzzy self-tuning PID controller.

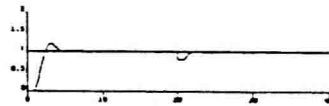


Figure 5: The response of the PID controller using the Ziegler- Nichols formula, where $K_c = 1.8$, $T_i = 2.4$, $T_d = 0.6$.

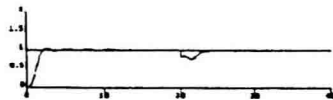


Figure 3: The response of the PID controller with dynamical neural networks.

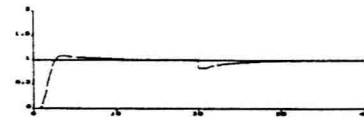


Figure 6: The response of the fuzzy self-tuning PID controller.



Figure 7: The response of the PID controller with dynamical neural networks.

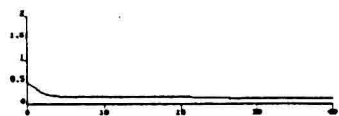


Figure 8: The parameter α .

disturbances exist. From simulation results, the performance of the proposed control scheme is compared favorably to those of the PID control scheme and the fuzzy self-tuning of PID control scheme.

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Control of a Static Nonlinear Plant Using a Neural Network Linearization

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Abstract — One possibility to control a static plant is the design of a controller based on the inverse of an identified model. For nonlinear plants, determining or identifying the plant model may be a difficult task. When a state space model of the plant is not explicitly needed, it is possible to consider the plant as a black box and approximate the plant using neural networks. In this paper a control strategy is presented, based on the combination of classical linear control methods with a neural network that inverts the plants nonlinear characteristics. A proof is given that the plant can be positioned with an arbitrary small positioning error. The method is experimentally illustrated on the positioning control of a flexible robot arm. The results of the neural network based control are compared with a PI controller.

1. Introduction

In the past few years, much effort has been put into the control of nonlinear robot arms. In general these arms are considered as flexible beams, for which the dynamics are identified, and an inverting controller is developed (see [6] ... [8]). In our problem, the manipulator kinematics are strongly nonlinear, such that the kinematics could not easily be identified. The goal here is to find a control force that can position the spring manipulator accurately to any point within a given work space, called the *region of interest*.

In a first attempt to solve the identification problem, a nonlinear model of the plant was constructed. The spring was modelled as a chain of flexible links. Benati [1] describes the equations of motion for such a chain. The same is done by Oliviers and Campion [9], with the remaining task of identifying the many parameters and finding the derivation of the inverse kinematics needed for control. In a more elaborate case where the manipulator has unresolved kinematics, it can become redundant [5] or hyper-redundant [2]. Hirose states in [5] that even in the redundant case, it is impossible to derive the inverse Jacobian matrix of the kinematics and dynamics.

A study on a nonlinear plant based on a pneumatic driven manipulator, was recently done by Hesselroth [4]. He put both the controller and the linearization scheme in one single black box.

This paper considers only the plant as a black box. Measurements are used to train an inverting neural network [10] off-line to linearize the plant. Next, a controller is designed using classical PI control. Section 2. of this paper will give the assumptions under which the control can be

mathematically described. Section 3. will give a practical example on the use of the control scheme.

2. Linearization using Neural Networks

2.1. Assumptions

Consider a static nonlinear plant h that maps an input $U \in \mathbb{R}^2$ to the output $Y \in \mathbb{R}^2$ with U and Y considered as column vectors: $U = [u_1 \ u_2]^T$ and $Y = [y_1 \ y_2]^T$ such that $y_i = h_i(U) = h_i(u_1, u_2)$; $i = 1, 2$.

Assumption 1: The plant h is locally linearizable in each point $U_0 \in \mathbb{R}^2$. Higher order derivatives of h are negligible compared to the first order derivative. This means that the plant is continuous and for any point U in a neighbourhood of U_0 yields:

$$h_i(U) \equiv h_i(U_0) + (\Delta U)^T \frac{\partial h_i(U_0)}{\partial U} \quad i = 1, 2 \quad (1)$$

$$\text{with } \Delta U = U - U_0 \text{ and } \frac{\partial h_i(U)}{\partial U} = \left[\frac{\partial h_i(U)}{\partial u_1} \quad \frac{\partial h_i(U)}{\partial u_2} \right]^T$$

Assumption 2: For each $U \in \Omega$ with $\Omega \subset \mathbb{R}^2$ corresponding to the region of interest of the robot arm, the first derivative of $h_i(U)$ exists and:

$$0 < \left| \frac{\partial h_i(U)}{\partial U} \right| < \infty \quad i = 1, 2 \quad (2)$$

Denote $\Psi \subset \mathbb{R}^2$ as the space of outputs related to Ω such that $Y \in \Psi$ and $U = h^{-1}(Y) = \begin{bmatrix} h_1^{-1}(y_1, y_2) \\ h_2^{-1}(y_1, y_2) \end{bmatrix}$

Based on a series of positioning measurements, a number of input-output pairs (U_i, Y_i) ; $i = 1 \dots N$ is taken. The inputs and outputs are restricted to the area of interest of the robot arm and are used to train a neural network to form a mapping $\tilde{h}^{-1}$ that inverts the relation $Y = h(U)$:

$$\tilde{h}^{-1}(Y): \Psi \rightarrow \Omega: \tilde{U} = \tilde{h}^{-1}(Y) = \begin{bmatrix} \tilde{h}_1^{-1}(y_1, y_2) \\ \tilde{h}_2^{-1}(y_1, y_2) \end{bmatrix} \quad (3)$$

Assumption 3: This inversion is not perfect and differs from the real inverting function $h^{-1}(Y)$ with an error $\delta h^{-1}(Y)$ that can be added to the real inverting function:

$$\tilde{h}_i^{-1}(Y) = h_i^{-1}(Y) + \delta h_i^{-1}(Y) \quad i = 1, 2 \quad (4)$$

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Assumption 4: The errors $\delta h_i^{-1}(Y)$ have an upper limit $\overline{\delta h^{-1}}$ such that for all $Y \in \Psi$ yields

$$\overline{\delta h^{-1}} = \max_{\substack{Y \in \Psi \\ i = 1, 2}} |\delta h_i^{-1}(Y)| \quad (5)$$

In practise $\overline{\delta h^{-1}}$ is determined from a validation set of input-output pairs $(U_j, Y_j); j = 1 \dots M$ that are also taken from the area of interest.

Assumption 5: For the neural network approximation $\tilde{h}^{-1}(Y)$, a class of neural network functions is used that are differentiable with respect to Y such that the first derivative $\frac{\partial \tilde{h}^{-1}(Y)}{\partial Y}$ can be calculated for all $Y \in \Psi$. This excludes the use of e.g. hard limit transfer functions or saturated linear transfer functions [3].

Assumption 6: The identification of the inverse of the plant $\tilde{h}^{-1}(Y)$ is done in such a way that within the area of interest, variations on the error are negligible with respect to variations on $h^{-1}(Y)$. The derivation of equation (4) then gives:

$$\forall Y \in \Psi; \frac{\partial \tilde{h}^{-1}(Y)}{\partial Y} \equiv \frac{\partial h^{-1}(Y)}{\partial Y} \quad (6)$$

or, also: for each Y in a neighbourhood of $\hat{Y}$ yields:

$$\delta h^{-1}(\hat{Y}) \equiv \delta h^{-1}(Y) \quad (7)$$

This assumption demands that the neural network does not only fit the surface, but also the slope of the surface at any point. This is the case as long as the neural network is not overparametrized.

Corollary 1: $h^{-1}(Y)$ and $\tilde{h}^{-1}(Y)$ are locally linear.

Proof: According to assumptions 1 and 2, $Y = h(U)$ is locally linearizable with finite, nonzero derivatives. Then also $U = h^{-1}(Y)$ is locally linearizable and from assumption 6 follows that $\tilde{h}^{-1}(Y)$ can be locally linearized. $\square$

Lemma 1: For an input $E = [e_1 \ e_2]^T$ the concatenation of the transfer functions $h(\tilde{h}^{-1}(E))$ can be written as

$$h_i[\tilde{h}^{-1}(E)] = e_i + \sum_{j=1,2} \delta h_j^{-1}(E) \frac{1}{\frac{\partial \tilde{h}_j^{-1}(E)}{\partial y_i}} \quad i = 1, 2 \quad (8)$$

Proof: With assumption 3, $h_i[\tilde{h}^{-1}(E)]$ can be written as

$$\begin{aligned} h_i[\tilde{h}^{-1}(E)] &= h_i(\tilde{h}_1^{-1}(E), \tilde{h}_2^{-1}(E)) \\ &= h_i(h_1^{-1}(E) + \delta h_1^{-1}(E), h_2^{-1}(E) + \delta h_2^{-1}(E)) \end{aligned} \quad (9)$$

and by assumption 1

$$h_i[\tilde{h}^{-1}(E)] = h_i(h_1^{-1}(E), h_2^{-1}(E)) +$$

$$\sum_{j=1,2} \delta h_j^{-1}(E) \frac{\partial h_i(h_1^{-1}(E), h_2^{-1}(E))}{\partial u_j} \quad (10)$$

corollary 1 states that h is locally linear and its derivative is finite (assumption 2). Therefore the derivative of the inverse of h exists and is nonzero. This gives:

$$h_i[\tilde{h}^{-1}(E)] = h_i(h_1^{-1}(E), h_2^{-1}(E)) +$$

$$\sum_{j=1,2} \delta h_j^{-1}(E) \frac{1}{\frac{\partial h_j^{-1}(E)}{\partial y_i}} \quad (11)$$

and by assumption 6

$$h_i[\tilde{h}^{-1}(E)] = e_i + \sum_{j=1,2} \delta h_j^{-1}(E) \frac{1}{\frac{\partial h_j^{-1}(E)}{\partial y_i}} \quad (12)$$

with $i = 1, 2 \quad \square$

2.2. Design of a Feedforward Control Scheme

An intuitive way to use the inverting function on the plant is to put it in sandwich between a linear controller G and the plant. Therefore consider the setup of Fig. 1.

The controller $G(t): \mathcal{R}^2 \rightarrow \mathcal{R}^2: U(t) = G(t) * \varepsilon(t)$, with $*$ the convolution in time, is not directly connected to the plant but separated by a feedforward linearizing function.

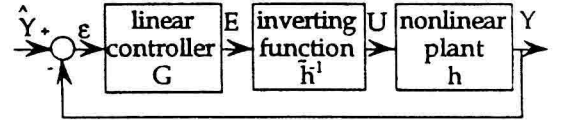


Figure 1. feedforward control scheme

This control scheme differs from many other neural network control schemes in the fact that the controller itself is not included in the neural network, as is the case in e.g. [4] and [11]. The closed loop relation is:

$$Y(t) = h(\tilde{h}^{-1}(G(t) * [\hat{Y} - Y(t)])) \quad (13)$$

Assumption 7: The bandwidth of $[\hat{Y} - Y(t)]$ is very small compared to that of the controller G such that $G(t) * [\hat{Y} - Y(t)]$ can be approximated by a plain multiplication $G(t)[\hat{Y} - Y(t)]$. For this, both the bandwidths of the setpoint $\hat{Y}$ and the plant h are expected to be very small compared to the bandwidth of the controller G . This assumption is based upon the observation that in our case the robot arm moves very slowly and is heavily damped.

Hence, equation (13) can be written as:

$$Y(t) \equiv h(\tilde{h}^{-1}(G(t)[\hat{Y} - Y(t)])) \quad (14)$$

in which G decouples the control of $h_1(E)$ and $h_2(E)$:

$$G(t) = \begin{bmatrix} g_{1,1}(t) & 0 \\ 0 & g_{2,2}(t) \end{bmatrix} = \begin{bmatrix} g_1(t) \\ g_2(t) \end{bmatrix} \quad (15)$$

Applying Lemma 1 on equation (14) gives:

$$\begin{aligned} y_i(t) &= e_i + \sum_{j=1,2} \delta h_j^{-1}(E(t)) \frac{1}{\frac{\partial \tilde{h}_j^{-1}(E(t))}{\partial y_i}} \\ &= \frac{g_{i,i}(t)}{1 + g_{i,i}(t)} \hat{y}_i(t) + \Delta y_i(t) \quad i = 1, 2 \end{aligned} \quad (16)$$

with $E(t)$ defined as $E(t) = G(t)(\hat{Y} - Y(t))$. It can be shown that the error $\Delta y_i(t)$ becomes a complex function in which both $\delta h_i^{-1}(Y)$ and $\frac{\partial \tilde{h}_i^{-1}(Y)}{\partial y_i}$ are applied on $E(t)$.

The possibility exists that $E(t) = G(t)(\hat{Y} - Y(t)) \notin \Psi$, hence the neural network is excited outside the region of interest. The results of this extrapolation of the neural network mapping are uncertain and may lead to instabilities or uncontrolled modes on the output U . Therefore, an alternative setup is considered in the next section.

2.3. Design of a Feedback Control Scheme

An alternative setup is shown in Fig. 2. The linear controller $G(t): \mathcal{R}^2 \rightarrow \mathcal{R}^2: U(t) = G(t) * \varepsilon(t)$ is directly connected to the nonlinear plant and the inverting function is put into the feedback loop. The setpoint $\hat{Y}$ is inverted using the same neural network to become a corrected setpoint $\hat{\kappa}$.

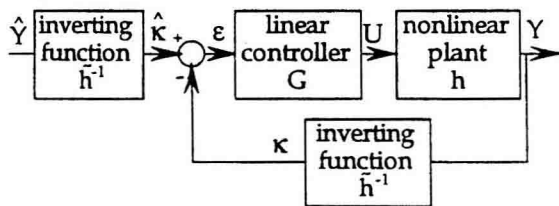


Figure 2. feedback control scheme

$G(t)$ is determined from the closed loop relation:

$$Y(t) = h(G(t) * [\tilde{h}^{-1}(\hat{Y}) - \tilde{h}^{-1}(Y(t))]) \quad (17)$$

With assumption 7 this becomes:

$$h_i^{-1}(Y(t)) = g_{i,i}(t) [\tilde{h}_i^{-1}(\hat{Y}) - \tilde{h}_i^{-1}(Y(t))] \quad i = 1, 2 \quad (18)$$

$$g_{i,i}(t) = \frac{h_i^{-1}(Y(t))}{\tilde{h}_i^{-1}(\hat{Y}) - \tilde{h}_i^{-1}(Y(t))} \quad i = 1, 2 \quad (19)$$

2.4. Feedback control scheme convergence analysis

Lemma 2: It is always possible to control the output

$Y(t)$ of the nonlinear plant in Fig. 2 to any desired state $\hat{Y} \in \Psi$ with a maximum error

$$|\Delta \hat{y}_i(t)| \leq \bar{\delta} h^{-1} \sum_{j=1,2} \left| \frac{1}{\frac{\partial \tilde{h}_j^{-1}(\hat{Y})}{\partial y_i}} \right| \quad i = 1, 2 \quad (20)$$

Proof: Break the closing loop in Fig. 2 and choose $g_{i,i} = 1$. The remaining network is a feed-forward control with output

$$Y(t) = h(\tilde{h}^{-1}(\hat{Y})) \quad (21)$$

Using Lemma 1 gives

$$\begin{aligned} h_i(\tilde{h}^{-1}(\hat{Y})) &= \hat{y}_i + \sum_{j=1,2} \delta h^{-1}(\hat{Y}) \frac{1}{\frac{\partial \tilde{h}_j^{-1}(\hat{Y})}{\partial y_i}} \quad i = 1, 2 \quad (22) \\ &= \hat{y}_i + \Delta \hat{y}_i(t) \end{aligned}$$

Following assumption 4 it is possible to find an upper bound for the error δh^{-1} , giving the inequality of equation (20). $\square$

Lemma 3: The nonlinear plant in Figure 2. can be globally controlled to any $\hat{Y} \in \Psi$ with an arbitrary small error.

Proof: Following Lemma 2 the output $Y(t)$ of the plant can be controlled to within a neighbourhood of $\hat{Y}$ as given in equation (20). At that point the feedback loop is closed and the gain G of the controller is taken as in equation (19).

Use corollary 1 on equation (19) and replace the exact inverting function by its neural network approximation. Then it can be proven that the discrete time update G^k at every time step k , can be calculated as:

$$g_{i,i}^k \geq \left| \frac{\tilde{h}_i^{-1}(Y^k)}{\bar{\delta} h^{-1} M} \right| \quad (23)$$

This will lead us to the following assumption:

Assumption 8: $g_{i,i}(t)$ is assumed to be much larger than 1 at any time during the control, or $g_{i,i}^k \gg 1$.

This assumption is based on the fact that the value $\tilde{h}_i^{-1}(Y^k) / \bar{\delta} h^{-1}$ is related to the maximum relative error of the neural network with respect to the input-output pairs that were used for training, while the goal of the training is to make the maximum error $\bar{\delta} h^{-1}$ as small as possible.

Starting from the closed loop equation (18) and using assumption 3 on $\tilde{h}_i^{-1}(Y)$, we can write:

$$h_i^{-1}(Y) = g_{i,i}(\tilde{h}_i^{-1}(\hat{Y}) - h_i^{-1}(Y) - \delta h_i^{-1}(Y)) \quad (24)$$

or, more in general:

$$Y = h(\tilde{h}^{-1}(\hat{Y})) - (I + G)^{-1} \tilde{h}^{-1}(\hat{Y}) - G(I + G)^{-1} \delta h^{-1}(Y) \quad (25)$$

The right two terms are significantly smaller than $\tilde{h}^{-1}(\hat{Y})$ since G is taken very large (assumption 8) and δh^{-1} is known to be very small. Therefore assumption 1 applies, and we can write equation (25) as:

$$Y = h(\tilde{h}^{-1}(\hat{Y})) - [(I + G)^{-1} \tilde{h}^{-1}(\hat{Y}) + G(I + G)^{-1} \delta h^{-1}(Y)] \tau \frac{\partial h(\tilde{h}^{-1}(\hat{Y}))}{\partial U} \quad (26)$$

Lemma 1 applies on $h(\tilde{h}^{-1}(\hat{Y}))$, such that

$$Y = \hat{Y} + (\delta h^{-1}(\hat{Y})) \tau \frac{\partial h(\tilde{h}^{-1}(\hat{Y}))}{\partial U} - (\delta h^{-1}(Y)) \tau \frac{\partial h(\tilde{h}^{-1}(\hat{Y}))}{\partial U} + [(I + G)^{-1} \delta h^{-1}(Y) - (I + G)^{-1} \tilde{h}^{-1}(\hat{Y})] \tau \frac{\partial h(\tilde{h}^{-1}(\hat{Y}))}{\partial U} \quad (27)$$

Assumption 6 gives that $\delta h^{-1}(\hat{Y}) \equiv \delta h^{-1}(Y)$ and using corollary 1:

$$y_i = \hat{y}_i + \frac{1}{1 + g_{i,i}} (\delta h_i^{-1}(Y) - \tilde{h}_i^{-1}(\hat{Y})) \sum_{j=1,2} \frac{1}{\frac{\partial \tilde{h}_j^{-1}(\hat{Y})}{\partial y_i}} \quad (28)$$

$$= \hat{y}_i + \Delta \hat{y}_i$$

The upper bound on $\delta h_i^{-1}(Y)$ is known (assumption 4) such that the upper bound on the final positioning error $\Delta \hat{y}_i$ can be calculated as:

$$\Delta \hat{y}_i \leq \frac{1}{1 + g_{i,i}} (\delta \tilde{h}^{-1} + |\tilde{h}_i^{-1}(\hat{Y})|) \sum_{j=1,2} \frac{1}{\left| \frac{\partial \tilde{h}_j^{-1}(\hat{Y})}{\partial y_i} \right|} \quad (29)$$

The upper limit for the positioning error can be chosen by increasing the gain $g_{i,i}$. $\square$

2.5. Remarks

A few practical conclusions for feedback control must be considered:

- $g_{i,i}$ can not always be taken arbitrarily high. In practise the gain is limited by the motor drivers, but also by the theoretical demand that $U \in \Omega$, such that $Y \in \Psi$ can be strictly guaranteed.
- In the case that h^{-1} is flattening (e.g. for nonlinear systems with higher order terms), feedback control showed to be noise sensitive. The reason lays mainly in the fact that output noise is hidden for the controller.

- If the assumption $\delta h^{-1}(\hat{Y}) \equiv \delta h^{-1}(Y)$ can not be made, the resulting output error will be limited to $\Delta Y < |h(\delta h^{-1}(\hat{Y}) - \delta h^{-1}(Y))|$. After convergence, a static error will remain that mainly depends on the quality of the neural network mapping.

3. Experimental Example

3.1. Description of the plant

A helicoidal spring is contracted using two computer controlled pulling cables K and L , that are connected at regular intervals inside the coil. The connections allow the cable to slide through in order to reduce the force between a cable and a section to radial components. By pulling the two cables, the spring bends over to a side and can be positioned at any point of a region in a 2-dimensional plane. This region is the region of interest Ψ of the plant.

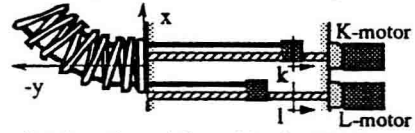


Figure 3. Mounting of the cables inside the spring setup

The motor speed values are updated by a Matlab routine that contains the controller in software. Due to the friction of the cables inside the spring, and low motor speeds, the spring can be considered as fully damped.

Starting from a random set of (Y_i, U_i) measurements it is possible to determine a (k, l) phase plane with measured motor positions. Ω is chosen as:

$$\Omega \subset \mathbb{R}^2: U_i \in \Omega; U_i = (k, l) \quad (30)$$

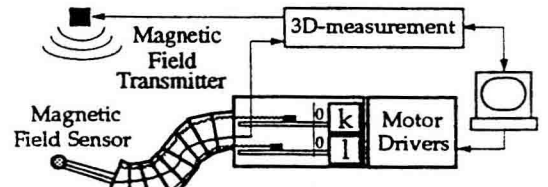


Figure 4. Measurement setup

The two motors cannot be placed at arbitrary positions. If one spindle would be placed at the far end while the other is fully pulled back, the spring would bend too far and the setup can get damaged. From the measurements it is possible to determine a (k, l) plane with static motor positions that will keep the end tip in a safe region of the measurement setup. This plane is used as a software bound for the motors in order to guarantee a safe operation of the spring.

3.2. A first approach using plain PI control

For reasons of comparison, the spring is controlled using